

# CLC420

## High Speed, Voltage Feedback Op Amp

### General Description

The CLC420 is an operational amplifier designed for applications requiring matched inputs, integration or transimpedance amplification. Utilizing voltage feedback architecture, the CLC420 offers a 300MHz bandwidth, a 1100V/ $\mu$ s slew rate and a 4mA supply current (power consumption of 40mW,  $\pm$ 5V supplies).

Applications such as differential amplifiers will benefit from 70dB common mode rejection ratio and an input offset current of 0.2 $\mu$ A. With its unity-gain stability, 2pA/ $\sqrt$ Hz current noise and 3 $\mu$ A of input bias current, the CLC420 is designed to meet the needs of filter applications and log amplifiers. The low input offset current and current noise, combined with a settling time of 18ns to 0.01% make the CLC420 ideal for D/A converters, pin diode receivers and photo multipliers amplifiers. All applications will find 70dB power supply rejection ratio attractive.

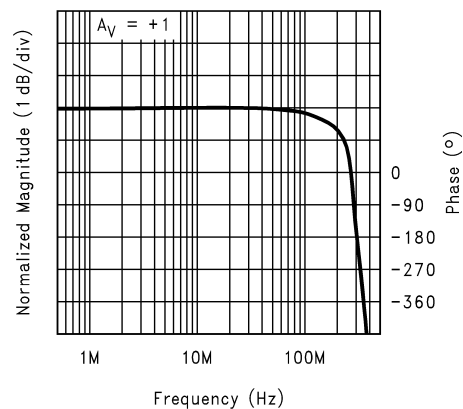
### Features

- 300MHz small signal bandwidth
- 1100V/ $\mu$ s slew rate
- Unity-gain stability
- Low distortion, -60dBc at 20MHz
- 0.01% settling in 18ns
- 0.2 $\mu$ A input offset current
- 2pA/ $\sqrt$ Hz current noise

### Applications

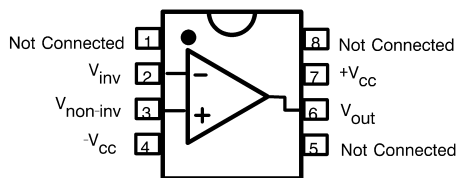
- Active filters/integrators
- Differential amplifiers
- Pin diode receivers
- Log amplifiers
- D/A converters
- Photo multiplier amplifiers

**Non-Inverting Frequency Response**



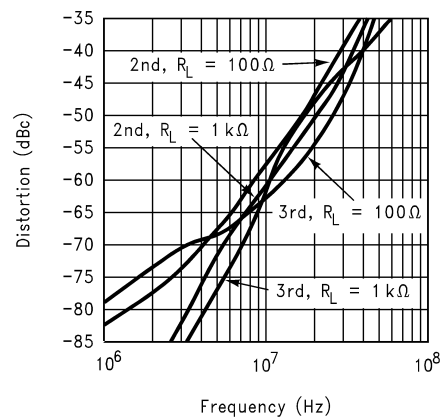
DS012752-19

### Connection Diagram



DS012752-18

**Pinout  
DIP & SOIC**



DS012752-20

**2nd and 3rd Harmonic Distortion**

**Ordering Information**

Package	Temperature Range Industrial	Part Number	Package Marking	NSC Drawing
8-pin plastic DIP	-40°C to +85°C	CLC420AJP	CLC420AJP	N08E
8-pin plastic SOIC	-40°C to +85°C	CLC420AJE	CLC420AJE	M08A
		CLC420AJE-TR13	CLC420AJE	

**Absolute Maximum Ratings** (Note 1)

If Military/Aerospace specified devices are required, please contact the National Semiconductor Sales Office/Distributors for availability and specifications.

Supply Voltage ( $V_{CC}$ )	$\pm 7V$
$I_{OUT}$ (is short circuit protected to ground, but maximum reliability will be maintained if $I_{OUT}$ does not exceed 70mA, except A8D, B8D which should not exceed 35mA over the military temperature range)..	70mA
Common Mode Input Voltage	$\pm V_{CC}$

Differential Input Voltage	10V
Junction Temperature	+150°C
Operating Temperature Range	-40°C to +85°C
Storage Temperature Range	-65°C to +150°C
Lead Solder Duration (+300°C)	10 sec

**Operating Ratings**

Thermal Resistance		
Package	( $\theta_{JC}$ )	( $\theta_{JA}$ )
MDIP	65°C/W	120°C/W
SOIC	60°C/W	140°C/W

**Electrical Characteristics**

$A_V = +1$ ,  $V_{CC} = \pm 5V$ ,  $R_L = 100\Omega$ ,  $R_f = 0\Omega$ ; unless specified

Symbol	Parameter	Conditions	Typ	Max/Min (Note 2)			Units
Ambient Temperature		CLC420AJ	+25°C	-40°C	+25°C	+85°C	
<b>Frequency Domain Response</b>							
SSBW	-3dB Bandwidth	$V_{OUT} < 0.4V_{PP}$	300	>200	>200	>130	MHz
LSBW		$V_{OUT} < 5V_{PP}$	40	>20	>25	>20	MHz
SSBWI	$A_V = -1$ , $R_f = 500\Omega$	$V_{OUT} < 0.4V_{PP}$	100	>65	>65	>45	MHz
LSBWI	$A_V = -1$ , $R_f = 500\Omega$	$V_{OUT} < 5V_{PP}$	60	>30	>35	>30	MHz
	Gain Flatness	$V_{OUT} < 0.4V_{PP}$					
GFPL	Peaking	0.1MHz to 100MHz	0	<1	<0.6	<0.6	dB
GFPH	Peaking	>100MHz	0	<5	<3	<3	dB
GFR	Rolloff	0.1MHz to 100MHz	0.2	<1	<1	<2	dB
GFRI	Rolloff, $A_V = -1$ , $R_f = 500\Omega$	0.1MHz to 30MHz	0.2	<1.4	<1.4	<1.6	dB
LPD	Linear Phase Deviation	0.1MHz to 100MHz	0.9	<1.8	<1.8	<2.5	deg
<b>Time Domain Response</b>							
TRS	Rise and Fall Time	0.4V Step	1.2	<2	<2	<3	ns
TRL		5V Step	1.4	<25	<20	<20	ns
TRSI	Rise and Fall Time, $A_V = -1$ , $R_f = 500\Omega$	0.4V Step	3.5	<5.5	<5.5	<7.8	ns
TRLI		5V Step	6	<10	<9.5	<10	ns
TSS	Settling Time to $\pm 0.1\%$	2V Step	12	<18	<18	<18	ns
TSP	$\pm 0.01\%$	2V Step	18	<25	<25	<25	ns
OS	Overshoot	0.4V Step	8	<35	<25	<25	%
SR	Slew Rate, $A_V = +2$	5V Step	1100	>600	>750	>600	V/ $\mu$ s
SRI	Slew Rate, $A_V = -1$ , $R_f = 500\Omega$	5V Step	750	>430	>500	>430	V/ $\mu$ s
<b>Distortion And Noise Response</b>							
HD2	2nd Harmonic Distortion	$2V_{PP}$ , 20MHz	-50	<-40	<-40	<-40	dBc
HD3	3rd Harmonic Distortion	$2V_{PP}$ , 20MHz	-53	<-45	<-45	<-40	dBc
HD2	2nd Harmonic Distortion	$A_V = -1$ $2V_{PP}$ , 20MHz, $R_f = 500\Omega$	-51	<-40	<-40	<-40	dBc
HD3	3rd harmonic distortion	$A_V = -1$ , $R_f = 500\Omega$ $2V_{PP}$ , 20MHz, $R_f = 500\Omega$	-51	<-40	<-40	<-35	dBc
	Input Referred Noise						
VN	Voltage	1MHz to 200MHz	4.2	<5.3	<5.3	<6	nV/ $\sqrt{Hz}$
ICN	Current	1MHz to 200MHz	2	<2.9	<2.6	<2.3	pA/ $\sqrt{Hz}$
<b>Static DC Performance</b>							
VIO	Input Offset Voltage (Note 3)		1	<3.2	<2	<3.5	mV

## Electrical Characteristics (Continued)

$A_V = +1$ ,  $V_{CC} = \pm 5V$ ,  $R_L = 100\Omega$ ,  $R_f = 0\Omega$ ; unless specified

Symbol	Parameter	Conditions	Typ	Max/Min (Note 2)			Units
<b>Static DC Performance</b>							
DVIO	Average Temperature Coefficient		8	<15	-	<15	$\mu V/^\circ C$
IB	Input Bias Current (Note 3)		3	<20	<10	<10	$\mu A$
DIB	Average Temperature Coefficient		45	<120	-	<60	$nA/^\circ C$
IIO	Input Offset Current (Note 3)		0.2	<2.6	<1	<2	$\mu A$
DIIO	Average Temperature Coefficient		2	<20	-	<10	$nA/^\circ C$
AOL	Open Loop Gain (Note 3)		65	>52	>56	>56	$\mu A$
PSRR	Power Supply Rejection Ratio		70	>55	>60	>60	dB
CMRR	Common Mode Rejection Ratio		80	>60	>65	>65	dB
ICC	Supply Current (Note 3)	No Load, Quiescent	4	<5	<5	<5	mA
<b>Miscellaneous Performance</b>							
RIND	Differential Mode Input	Resistance	2	>0.5	>1	>1	$M\Omega$
CIND		Capacitance	1	<2	<2	<2	pF
RINC	Common Mode Input	Resistance	1	>0.25	>0.5	>0.5	$M\Omega$
CINC		Capacitance	1	<2	<2	<2	pF
RO	Output Impedance	At DC	0.02	<0.3	<0.2	<0.2	$\Omega$
VO	Output Voltage Range	No Load	$\pm 3.6$	$\pm 2.8$	$\pm 3$	$\pm 3$	V
VOL	Output Voltage Range	$R_L = 100\Omega$	$\pm 2.9$	$\pm 2.5$	$\pm 2.5$	$\pm 2.5$	V
CMIR	Common Mode Input Range	For Rated Performance	$\pm 3.2$	$\pm 2.5$	$\pm 2.8$	$\pm 2.8$	V
IO	Output Current		$\pm 60$	$\pm 30$	$\pm 50$	$\pm 50$	mA

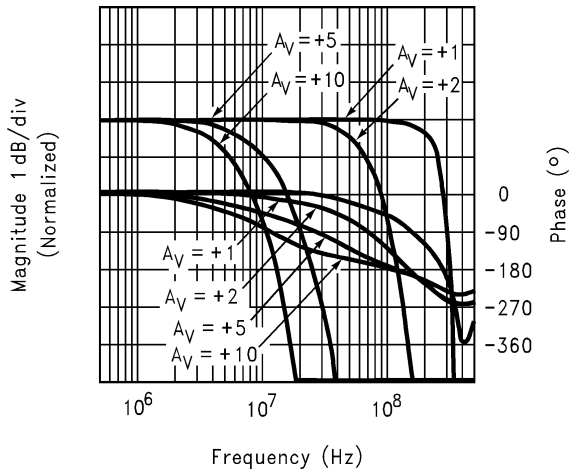
**Note 1:** "Absolute Maximum Ratings" are those values beyond which the safety of the device cannot be guaranteed. They are not meant to imply that the devices should be operated at these limits. The table of "Electrical Characteristics" specifies conditions of device operation.

**Note 2:** Max/min ratings are based on product characterization and simulation. Individual parameters are tested as noted. Outgoing quality levels are determined from tested parameters.

**Note 3:** AJ-level: spec. is 100% tested at  $+25^\circ C$ .

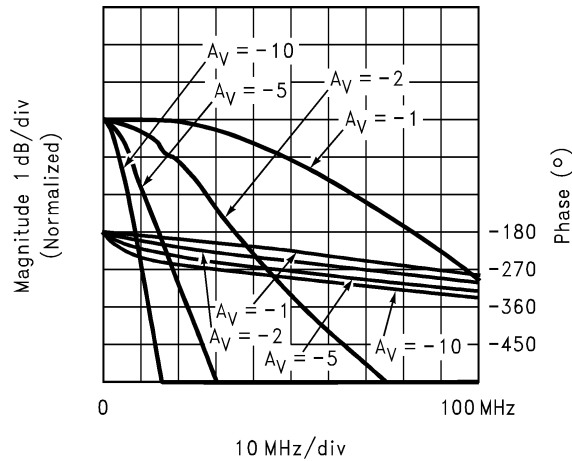
# Typical Performance Characteristics

## Non-Inverting Frequency Response



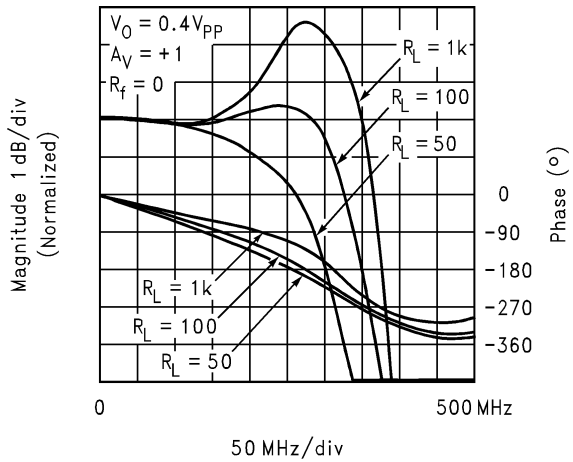
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## Inverting Frequency Response



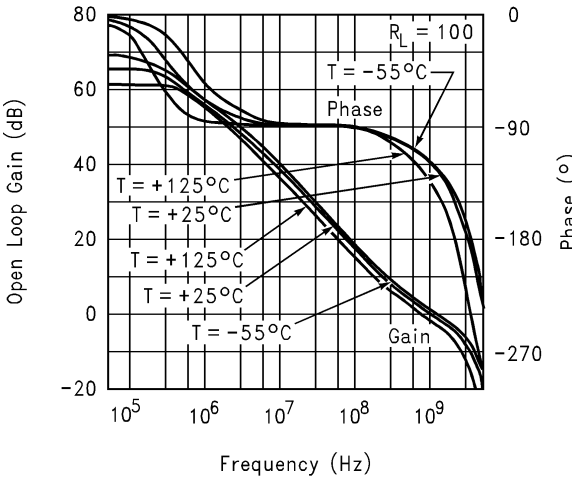
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## Frequency Response for Various $R_L$ 'S



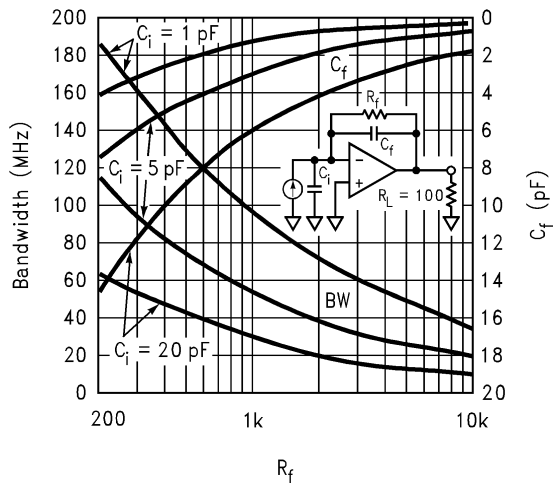
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## Open Loop Gain and Phase



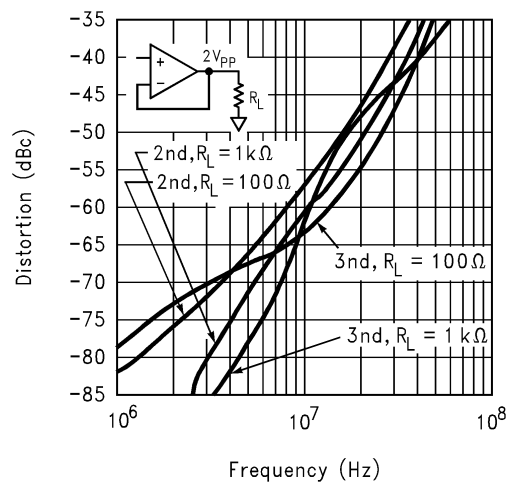
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## Bandwidth vs. Gain, Transimpedance Configuration



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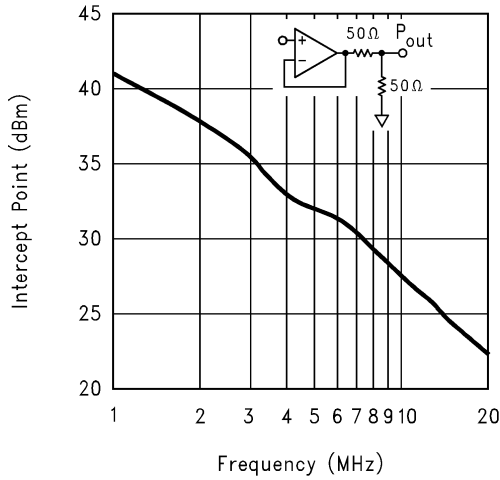
## 2nd and 3rd Harmonic Distortion



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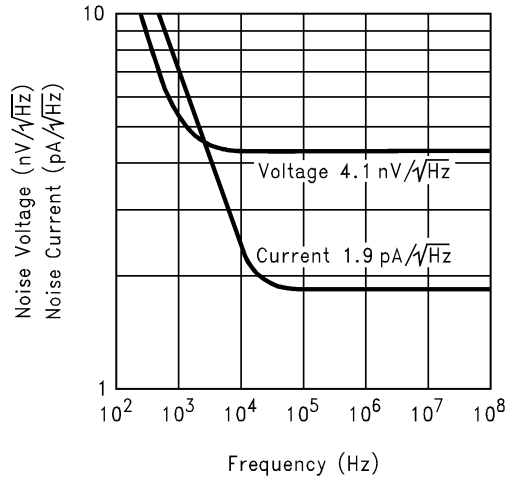
# Typical Performance Characteristics (Continued)

2-Tone, 3rd Order Intermodulation Intercept



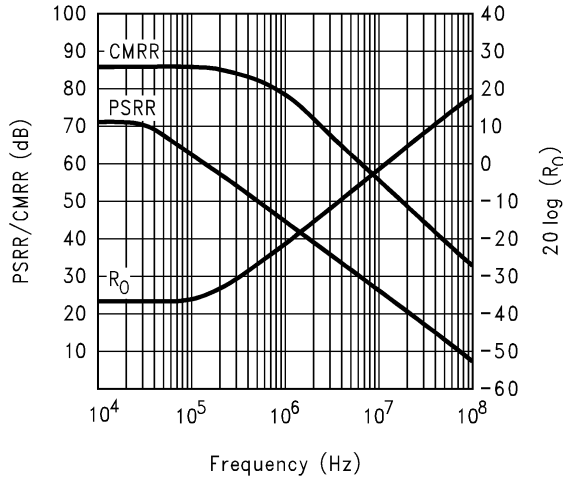
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Equivalent Input Noise



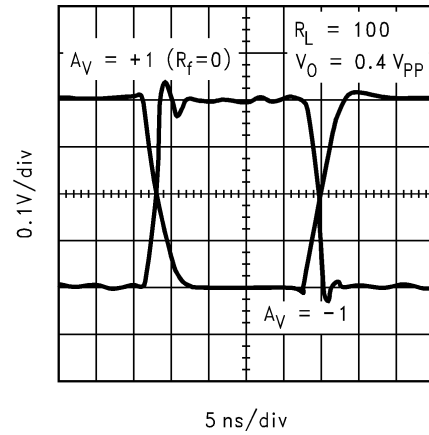
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PSRR, CMRR, and Closed Loop R<sub>O</sub>



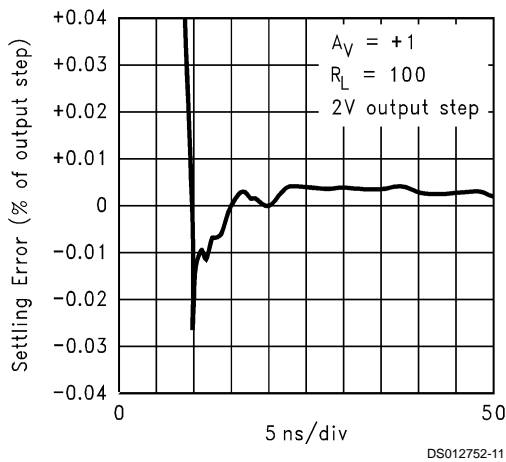
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Pulse Response



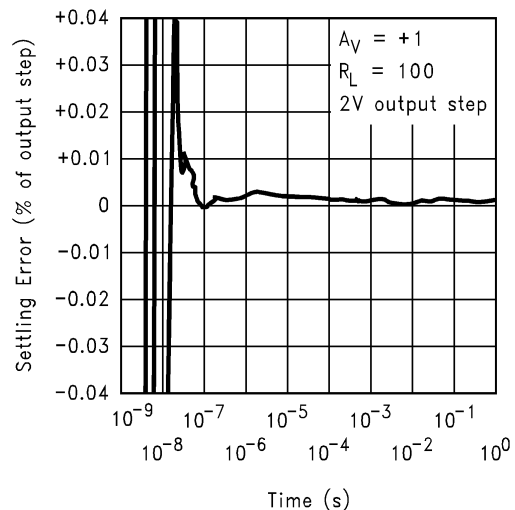
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Settling Time



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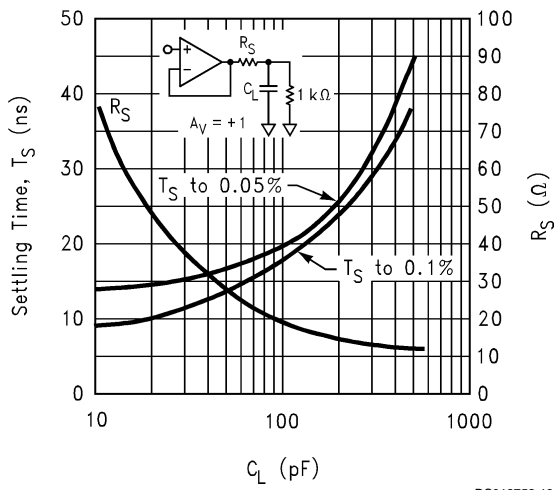
Long-Term Settling Time



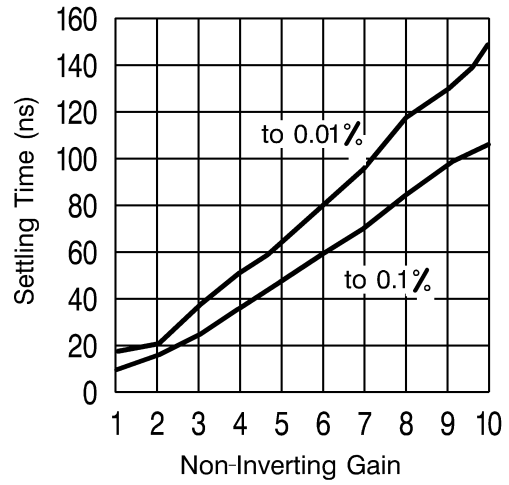
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# Typical Performance Characteristics (Continued)

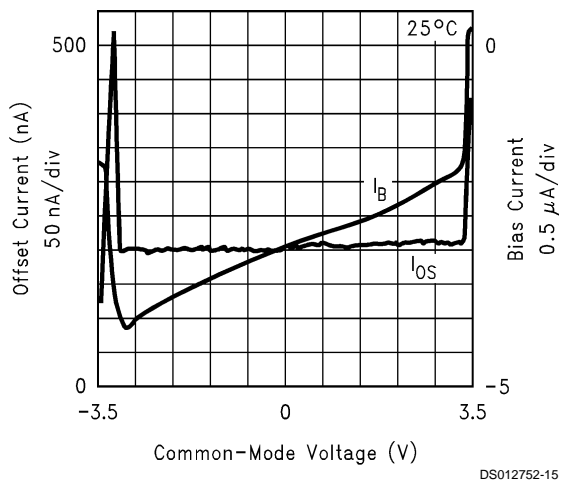
Settling Time vs. Capacitive Load



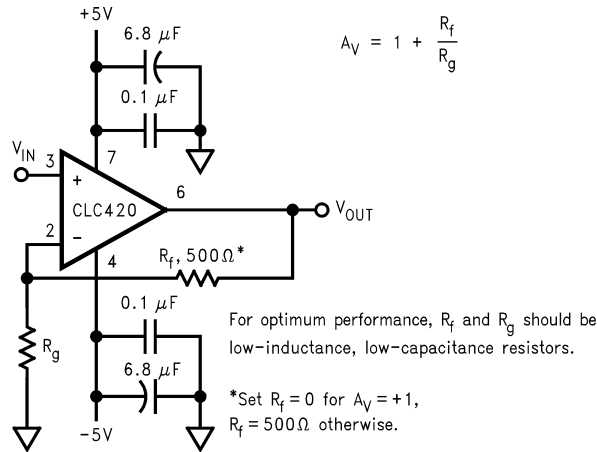
Settling Time vs. Gain



$I_B$  and  $I_{OS}$  vs. Common-Mode Voltage

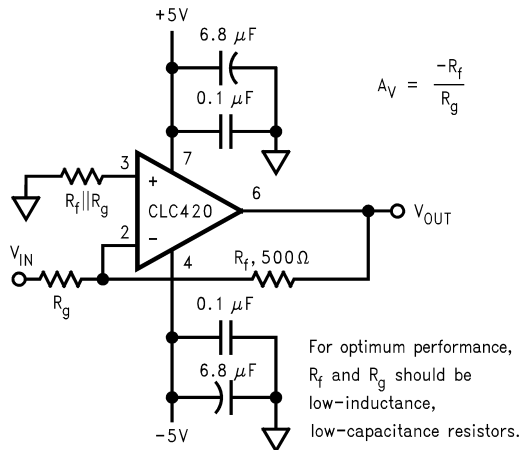


## Application Division



DS012752-16

FIGURE 1. Recommended Non-Inverting Gain Circuit



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FIGURE 2. Recommended Inverting Gain Circuit

**Description**

The CLC420 is a high speed, slew boosted, voltage feedback amplifier with unity-gain stability. These features along with matched inputs, low input bias and noise currents, and excellent CMRR render the CLC420 very attractive for active filters, differential amplifiers, log amplifiers, and transimpedance amplifiers.

**DC accuracy**

Unlike current feedback amplifiers, voltage-feedback amplifiers have matched inputs. This means that the non inverting and inverting input bias current are well matched and track over temperature, etc. As a result, by matching the resistance looking out of the two inputs, these errors can be reduced to a small offset current term.

**Gain bandwidth product**

Since the CLC420 is a voltage feedback op amp, closed loop bandwidth is approximately equal to the gain bandwidth product (typically 100MHz) divided by the noise gain of the circuit (for noise gains greater than 5). At lower noise gains, higher order amplifier poles contribute to higher closed loop bandwidth. At low gains use the frequency response performance plots given in the data sheet.

Another point to remember is that the closed loop bandwidth is determined by the noise gain, not the signal gain of the circuit. Noise gain is the reciprocal of the attenuation in the feedback network enclosing the op amp. For example, a CLC420 setup as a non-inverting amplifier with a closed loop gain of +1 (a noise gain of 1) has a 300MHz bandwidth. When used as an inverting amplifier with a gain of -1 (a noise gain of 2), the bandwidth is less, typically only 100MHz.

**Full-power bandwidth, and slew-rate**

The CLC420 combines exceptional full power bandwidths (40MHz,  $V_o = 5V_{pp}$ ,  $A_V = +1$ ) and slew rates (1100V/ $\mu$ s,  $A_V = +1$ ) with low (40mW) power consumption. These attractive results are achieved by using slew boosting circuitry to keep the slew rates high while consuming very little power.

In non slew boosted amplifiers, full power bandwidth can be easily determined from slew rate measurements, but in slew boosting amplifiers, such as the CLC420, you can't. For this reason we provide data for both.

Slew rate is also different for inverting and non-inverting configurations. This occurs because common-mode signal voltages are present in non-inverting circuits but absent in inverting circuits. Once again data is provided for both.



## Application Division (Continued)

### Transimpedance amplifier circuits

Low inverting, input current noise ( $2\text{pA}\sqrt{\text{Hz}}$ ) makes the CLC420 ideal for high sensitivity transimpedance amplifier circuits for applications such as pin diode optical receivers, and detectors in receiver IFs. However, feedback resistors  $4\text{k}\Omega$  or greater are required if feedback resistor noise current is going to be less than the input current noise contribution of the op amp.

With feedback resistors this large, shunt capacitance on the inverting input of the op amp (from the pin diode, etc.) will unacceptably degrade phase margin causing frequency response peaking or oscillations a small valued capacitor shunting the feedback resistor solves this problem (Note: This approach does not work for a current-feedback op amp configured for transimpedance applications). To determine the value of this capacitor, refer to the "Transimpedance BW vs.  $R_f$  and  $C_i$ " plot.

For example, let's assume an optical transimpedance receiver is being developed. Total capacitance from the inverting input to ground, including the photodiode and strays is  $5\text{pF}$ . A  $5\text{k}\Omega$  feedback resistor value has been determined to provide best dynamic range based on the response of the photodiode and the range of incident optical powers, etc.

From the "Transimpedance BW vs.  $R_f$  and  $C_i$ " plot, using  $C_i = 5\text{pF}$  it is determined from the two curves labeled  $C_i = 5\text{pF}$ , that  $C_f = 1.5\text{pF}$  provides optimal compensation (no more than  $0.5\text{dB}$  frequency response peaking) and a  $-3\text{dB}$  bandwidth of approximately  $27\text{MHz}$ .

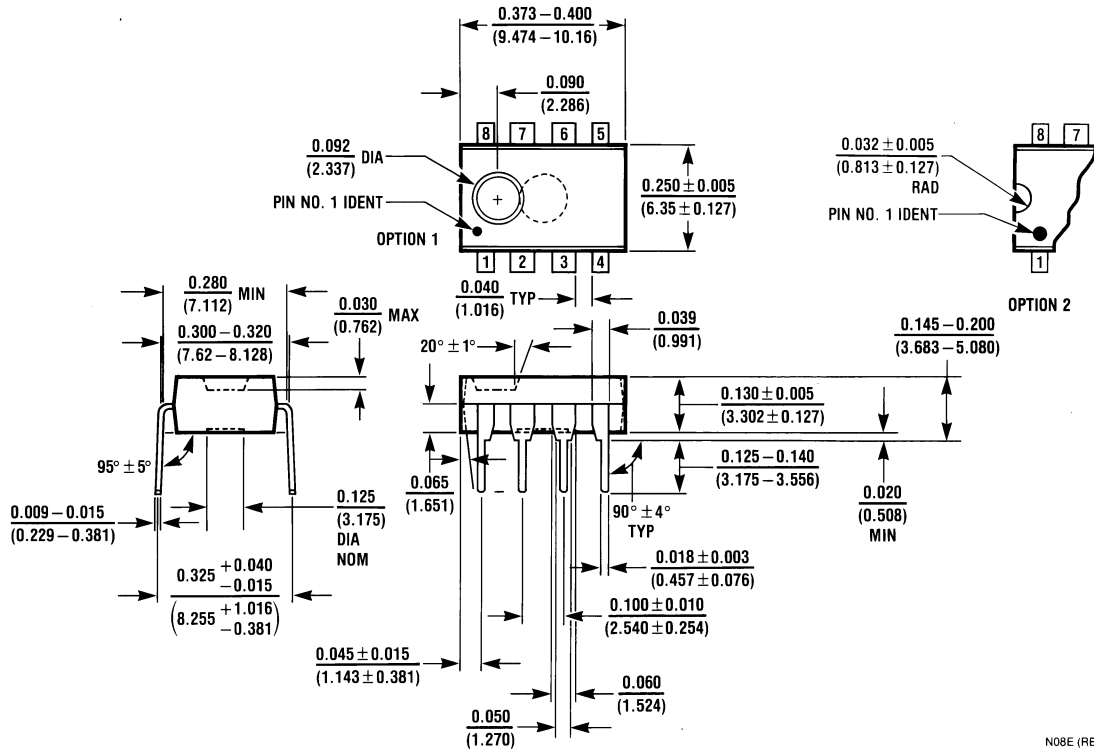
### Printed circuit layout

As with any high frequency device, a good PCB layout will enhance performance. Ground plane construction and good power supply bypassing close to the package are critical to achieving full performance. The amplifier is sensitive to stray capacitance to ground at the output and inverting input: Node connections should be small with minimal coupling to the ground plane.

Parasitic or load capacitance directly on the output (pin 6) will introduce additional phase shift in the loop degrading the loop phase margin and leading to frequency response peaking. A small series resistor before this capacitance, if present, effectively decouples this effect. The graphs on the preceding page, "Settling Time vs.  $C_L$ ", illustrates the required resistor value and resulting performance vs. capacitance.

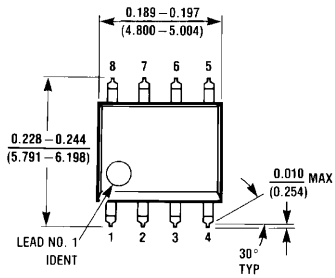
Evaluation PC boards (part no. 730013 for through-hole and CLC730027 for SOIC) are available for the CLC420.

**Physical Dimensions** inches (millimeters) unless otherwise noted



**8-Pin MDIP**  
NS Package Number N08E

N08E (REV F)



**8-Pin SOIC**  
NS Package Number M08A

M08A (REV H)

## Notes

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